

# Experimental Demonstration of High-Speed $4 \times 4$ Imaging Multi-CAP MIMO Visible Light Communications

Khald Werfli, Petr Chvojka, Zabih Ghassemlooy\*, Navid Bani Hassan, Stanislav Zvanovec, Andrew Burton, Paul Anthony Haigh, and Manav R. Bhatnagar

**Abstract**—In general, visible light communication (VLC) systems, which utilise white light-emitting diodes (LEDs), only offer a bandwidth limited to the lower MHz region. Therefore, providing VLC-based high data rate communications systems becomes a challenging task. To address this challenge, we propose a solution based on multiplexing in both the frequency and space domains. We experimentally demonstrate a  $4 \times 4$  imaging multiple-input multiple-output (MIMO) VLC system (i.e., space multiplexing) utilising multi-band carrier-less amplitude and phase (*m*-CAP) modulation (i.e., frequency multiplexing). Independently, both MIMO and *m*-CAP have shown the remarkable ability to improve transmission speeds in VLC systems, and hence, here we combine them to further improve the net data rate. We investigate link performance by varying the number of subcarriers  $m$ , link distance  $L$ , and signal bandwidth  $B_{sig}$ . From all the values tested, we show a data rate of ~249 Mb/s can be maximally achieved for  $m = 20$ ,  $B_{sig} = 20$  MHz, and  $L = 1$  m, at a bit error rate of  $3.2 \times 10^{-3}$  using LEDs with ~4 MHz bandwidth.

**Index Terms**—Modulation bandwidth, multi-band carrier-less amplitude and phase modulation, multiple-input multiple-output, visible light communications.

## I. INTRODUCTION

WIRELESS access technologies have continuously evolved in response to ever increasing capacity demands resulting from the wide spread use of smart and mobile devices. Current 4<sup>th</sup> generation wireless systems with a limited frequency spectrum will not be able to apportion sufficient bandwidth to cope with the exponentially growing traffic, and hence, highly spectrally efficient

communication techniques are one of the key considerations in research towards the 5<sup>th</sup> generation networks [1]. Within this context, visible light communications (VLC) can be used as a complementary wireless technology [2] to radio-frequency based schemes mostly in applications where high bandwidth  $B$  and low latencies are the main requirements. VLC has received growing research interest over the last decade; mostly due to the widespread use of light emitting diodes (LEDs) in solid-state lighting systems [3]. However, VLC systems have a number of challenges including (i) LEDs with limited bandwidths  $B_{LED}$  (typically  $< 5$  MHz, or higher for micro-LEDs); (ii) LED non-linearity; (iii) multipath induced inter-symbol interference (ISI); (iv) blocking and shadowing; and (v) limited mobility [3, 4], which limits the maximum achievable data rate  $R_b$  within a typical indoor environment.

Numerous number of schemes have been proposed to overcome these limitations [5-10]. As for the  $B_{LED}$  and ISI limitations, the most widely adopted schemes include pre- and post-equalizations, blue filtering, multiplexing and parallel transmission, and spectrally efficient modulation as well as multi-carrier transmission [11-13]. Of the latter, orthogonal frequency division multiplexing (OFDM) offers spectral efficiency only through compatibility with bit- and power-loading algorithms, thus enabling a higher number of bits/symbol/subcarrier [14, 15]. In [16-18] OFDM VLC links with  $R_b$  of several Gb/s were reported, and in [19] the aggregate  $R_b$  was increased to 3.4 Gb/s using a combination of OFDM and wavelength division multiplexing (WDM). Despite many advantages that OFDM offers, there are a number of drawbacks including (i) limited dynamic range; (ii) relatively high peak-to-average power ratio due to the LED nonlinearity [16-18]; and (iii) sensitivity to the carrier offset and drift, and phase noise, which results in lower overall spectral efficiency [20-22].

Alternatively, carrier-less amplitude and phase (CAP) modulation was shown to outperform OFDM in terms of  $R_b$  over the same transmission span  $L$  [23]. In [24], a CAP-VLC system employing a red-green-blue (RGB) LED and a hybrid post-equalizer was reported with  $R_b$  of 3.22 Gb/s. Overall, the CAP system based on intensity modulation and direct detection is less complex with improved performance compared to OFDM, which allows relatively higher  $R_b$  using optical and electrical components with limited  $B$  [25].

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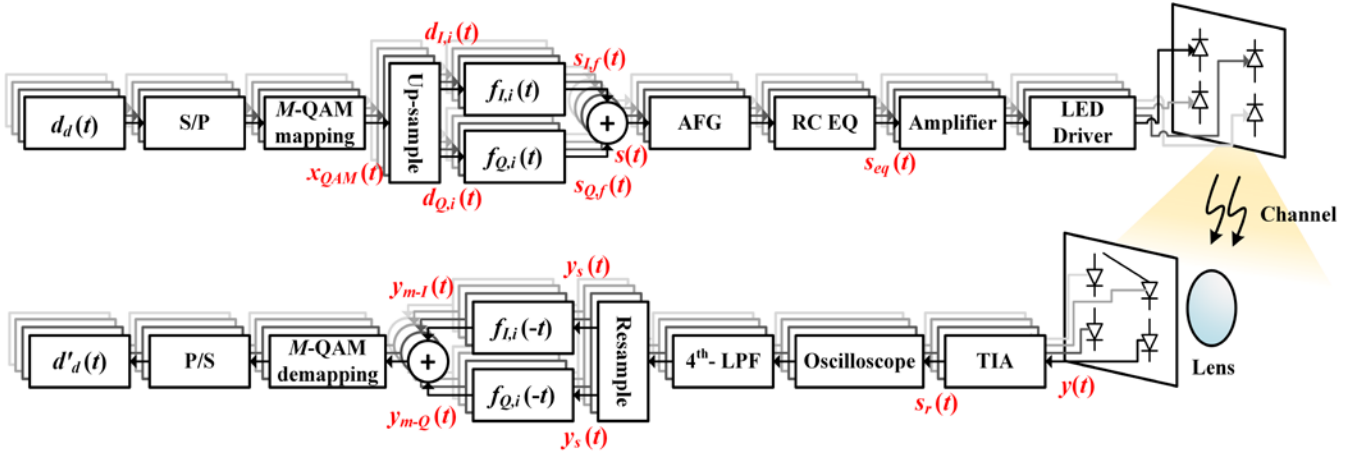


Fig. 1. The schematic block diagram of the 4 x 4 imaging MIMO  $m$ -CAP system

However, despite superior  $R_b$  and bit-error rate (BER) performance in comparison to OFDM, the major impediment in implementation of CAP VLC is that it is very sensitive to the high frequency attenuation [26], which is prevalent in VLC systems due to the LED frequency response (i.e., a low pass filter (LPF)). In [27] multi-band CAP ( $m$ -CAP) was first proposed for optical fibre communications prior to adoption by the VLC community [26], where the system bandwidth  $B_{\text{sys}}$  was evenly divided over  $m = 10$  subcarriers, each employing CAP with successively higher carrier frequencies over a low modulation bandwidth. It was found that a higher signal-to-noise ratio (SNR) per subcarrier could be supported due to the alleviation of the band-limiting conditions. Furthermore, the implementation of a bit-loading algorithm, which is not possible in 1-CAP, enabled the demonstration of a record (at the time of writing) spectral efficiency  $\eta_s$  of 4.85 b/s/Hz.

Simultaneously, the multiple-input multiple-output (MIMO) scheme can be adopted to increase the  $R_b$ . In indoor environments multiple LED-based lighting fixtures are used to provide sufficient illumination levels (i.e., 200-1000 lx [28]), which facilitates the implementation of MIMO-VLC [29]. An imaging MIMO-VLC system using micro-LEDs ( $B_{\text{LED}} > 20$  MHz) and  $R_b$  of  $\sim 920$  Mb/s over  $L$  of 1 m was experimentally demonstrated in [30]. In [31] an experimental  $4 \times 4$  optical non-imaging MIMO-VLC link with an aggregate  $R_b$  of 50 Mb/s over  $L$  of 2 m was demonstrated. In this work, for the first time, we experimentally demonstrate a  $4 \times 4$  imaging MIMO-VLC system based on  $m$ -CAP (i.e., a combination of frequency- and space-division multiplexing), and investigate the link's BER performance as a function of  $m$  (up to 20), a range of signal bandwidth  $B_{\text{sig}}$  and  $L$ . We also examine the net data rate  $R_{\text{net}}$  and the net spectral efficiency  $\eta_{\text{net}}$ , which shows that for a given  $m$  and  $L$ , increasing  $B_{\text{sig}}$  leads to an increase in  $R_{\text{net}}$  and reduced  $\eta_{\text{net}}$ . We demonstrate a maximum  $R_b$  of  $\sim 249$  Mb/s at a BER of  $3.2 \times 10^{-3}$ , given  $m = 20$ ,  $B_{\text{sig}} = 20$  MHz and  $L = 1$  m.

The rest of this paper is organised as follows: in Section II the system setup is described; results and discussions are shown in Section III, and finally, conclusions are drawn in Section IV.

## II. SYSTEM SETUP

As a proof of concept, Fig. 1 shows the schematic block diagram of the proposed experimental system, where  $m$  independent pseudorandom binary sequences (PRBS)  $d_d(t)$  in the non-return to zero (NRZ) format of length  $2^{17}-1$  are generated in the MATLAB domain. Following serial-to-parallel conversion (S/P),  $d_d(t)$  is then mapped onto the  $M$ -ary quadrature amplitude modulation ( $M$ -QAM) constellation symbols  $x_{QAM}(t)$ , where the cardinality is given by  $M = 2^b$  and  $b$  represents the number of bits/symbol.  $x_{QAM}(t)$  is then up-sampled by the number of samples/symbol  $n_{\text{samp}}$  as given by [27]:

$$n_{\text{samp}} = \lceil 2m(1 + \beta) \rceil, \quad (1)$$

where  $m$  represents the number of subcarriers, and  $\beta$  is the roll-off factor of the square root raised cosine (SRRC) filter, which is set to 0.15 for consistency with the literature [26, 27].

Both up-sampled signals  $d_{I,i}(t)$  and  $d_{Q,i}(t)$  of the  $i^{\text{th}}$  subcarrier are then passed through the real ( $I$ ) and imaginary ( $Q$ ) SRRC filters the outputs of which are given as [26]:

$$s_{I,f,i}(t) = d_{I,i}(t) \otimes f_{I,i}(t), \quad (2)$$

$$s_{Q,f,i}(t) = d_{Q,i}(t) \otimes f_{Q,i}(t), \quad (3)$$

where  $\otimes$  denotes time domain convolution,  $f_{I,i}(t)$  and  $f_{Q,i}(t)$  denote the impulse response of the  $I$  and  $Q$  SRRC filters of the  $i^{\text{th}}$  subcarrier, respectively, which are given by [32]:

$$f_{I,i}(t) = \cos(2\pi f_{c,i}t) \cdot \left[ \frac{\sin\left(\frac{\pi t}{T_s}(1 - \beta)\right) + 4\beta \frac{t}{T_s} \cos\left(\frac{\pi t}{T_s}(1 + \beta)\right)}{\frac{\pi t}{T_s}\left(1 - \left(4\beta \frac{t}{T_s}\right)^2\right)} \right], \quad (4)$$

$$f_{Q,i}(t) = \sin(2\pi f_{c,i}t) \cdot \left[ \frac{\sin\left(\frac{\pi t}{T_s}(1 - \beta)\right) + 4\beta \frac{t}{T_s} \cos\left(\frac{\pi t}{T_s}(1 + \beta)\right)}{\frac{\pi t}{T_s}\left(1 - \left(4\beta \frac{t}{T_s}\right)^2\right)} \right], \quad (5)$$

where  $T_s$  is the symbol duration. The carrier frequency for the  $i^{\text{th}}$  subcarrier is given by [33]:

$$f_{c,i} = \frac{(2i-1)B_{sig}}{2m}, \quad (6)$$

where  $B_{sig}$  is given by:

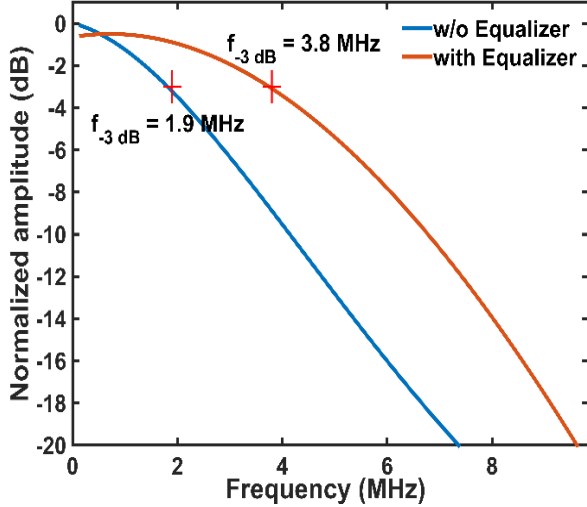


Fig. 3. LED frequency response with and without an equalizer

$$B_{sig} = \frac{1}{T_s} (1 + \beta)m. \quad (7)$$

Considering all subcarriers, the  $m$ -CAP output signal is given as [32]:

$$s(t) = \sqrt{2} \left( s_{I,f}(t) - s_{Q,f}(t) \right). \quad (8)$$

The  $m$ -CAP signal is then applied to identical arbitrary function generators (AFGs) using LabVIEW to generate the signals for the 4 spatial channels. The outputs  $s(t)$  of the four channels are sampled at 2 GS/s with a vertical resolution of 8-bit and is then passed through four independent resistor-capacitor based pre-equalizers (RC EQ) in order to extend  $B_{LED}$  from  $\sim 2$  MHz to 3.8 MHz, as shown in Fig. 2.

The four equalised signals  $s_{eq}(t)$  are then amplified (with a gain of 5 dB) prior to intensity modulation of LEDs (4 cool white 565K LUXEON Rebel LEDs) using a bias tee. Fig. 3 illustrates the experimental setup of the proposed system.

Note, the distances between the transmitter (Tx) and the lens  $L_t$  and between the lens and the optical receiver (Rx)  $L_r$ , respectively are given as:

$$L_t = f_l \frac{(\alpha - 1)}{\alpha}, \quad (9)$$

$$L_r = f_l(1 - \alpha), \quad (10)$$

where  $f_l$  is the lens focal length with a magnification factor given by [34]:

$$\alpha = -\frac{d_r}{d_t} = -\frac{L_r}{L_t}, \quad (11)$$

where  $d_r$  and  $d_t$  are the spacing between Rx's and Tx's, respectively.

Using the parameters given in Table I, the total link span  $L = L_t + L_r = 4.5f_l$ . For  $f_l$  of 0.25, 0.4 and 1 m,  $L$  are 1.125 m, 1.8 m and 4.5 m, respectively, which are representative dimensions for a typical indoor environment.

As shown in Fig. 3, at the Rx, a convex lens with a focal length  $f_l$  is used to focus the received optical beam of each channel onto its corresponding photodetectors (PDs) (silicon

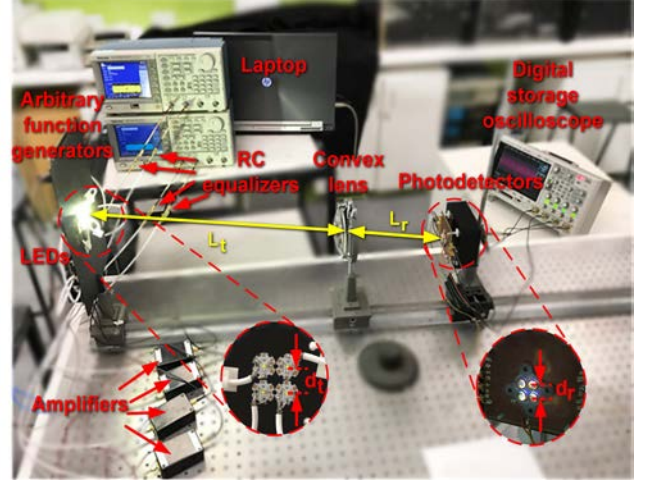


Fig. 2. Experimental setup. The convex lens is used to map the LEDs to the PDs. Spacing between Rx's and Tx's  $d_r$  and  $d_t$ , respectively

PD OSD15-5T) with a large enough surfacing area to capture the entire optical footprint. Therefore, with the proposed system being an imaging MIMO the lens employed at the Rx ensures that each PD receives the optical signal from its corresponding LED. As a result there are no inter-channel crosstalk as in [35], in contrast to the non-imaging MIMO VLC system, where additional signal processing and filtering are needed to mitigate the channel correlation between individual Tx's and Rx's, and inter-channel crosstalk.[35].

The received signal is given by:

Table I: SETUP AND PD PARAMETERS

Parameter	Value
Data-NRZ pseudorandom binary sequences length	$2^{17}-1$
Amplifier gain	5 dB
Convex lens	
• Focal length $f_l$	0.25 m, 0.40 m and 1 m
• Diameter $d$	110 mm, 105 mm and 50 mm
LED bandwidth $B_{LED}$	1.9 MHz
Photodetector - silicon OSD15-5T	
• Active area	15 mm <sup>2</sup>
• Responsivity $\mathcal{R}$	0.21 A/W
• Bandwidth $B_{PD}$	29 MHz
Spacing between Tx's $d_t$	0.01 m
Spacing between Rx's $d_r$	0.02 m
Signal bandwidth $B_{sig}$	5,10,15 and 20 MHz
Transmission span $L$	$\sim 1$ m, 1.8 m and 4.5 m

$$y(t) = \mathcal{R}s_{eq}(t) \otimes h(t) + n(t), \quad (12)$$

where  $h(t)$  is the channel impulse response,  $\mathcal{R}$  represents the PD's responsivity, and  $n(t)$  is the additive white Gaussian noise (AWGN). Note, the dominant noise sources are the ambient induced shots noise and the thermal noise, which are defined, respectively in terms of variances and is given as [28]:

$$\sigma_n^2 = 2qI_{bg}B_{Rx} + 4kTB_{Rx}, \quad (13)$$

where  $I_{bg}$  is the background light induced current,  $q$  is the electron charge,  $T$  is the absolute temperature,  $k$  is the Boltzmann's constant, and  $B_{Rx}$  is the receiver bandwidth.

A typical value for the thermal noise  $\sigma_{ther}^2 = 17.5348 \times 10^{-16} \text{ A}^2$  [36]. For a typical indoor environment the standard illumination level is between 300 - 500 lx at 0.8 m height from the floor level, which is equivalent to a power requirement of  $> 2.25 \times 10^{-4} \text{ W}$  [36]. This represents the shot noise variance of at least  $\sim 2 \times 10^{-16} \text{ A}^2$ , which is the same as  $\sigma_{ther}^2$ .

Following optoelectronic conversion and amplification using transimpedance amplifiers (TIAs), the regenerated electrical signals  $s_r(t)$  are captured using a digital storage oscilloscope (DSO-X3034A) with a sampling rate of 4 GS/s for off-line processing as outlined in the following paragraphs.  $s_r(t)$  is first passed through a 4<sup>th</sup> order Butterworth LPF with a cut-off frequency  $f_{cut} = B_{sig}$  [26] in order to reject the out-of-band noise. The filtered  $m$ -CAP signal is then resampled to match the transmitted sampling frequency prior to matched filtering, the output of which is given by:

$$y_{m-i}(t) = y_s(t) \otimes f_{i,i}(-t), \quad (14)$$

$$y_{m-q}(t) = y_s(t) \otimes f_{q,i}(-t), \quad (15)$$

where  $y_s(t)$  is the resampled signal.  $f_i(-t)$  and  $f_q(-t)$  are the impulse responses of the matched filters.

Following  $M$ -QAM demodulation and parallel-to-serial conversion (P/S) the estimated data symbols  $d'_d(t)$  are recovered. As reported in the literature, a binary phase shift keying based signal is first transmitted on each subcarrier to measure the error vector magnitude (EVM), prior to SNR estimation following the procedures adopted from [37, 38]:

$$\text{SNR}_i = 20 \log_{10} \left( \frac{\text{EVM}_{\text{RMS}_i}(\%) }{100} \right). \quad (16)$$

Next, a subcarrier-specific value of  $b$  is selected based on the estimated SNR. The proposed system performance is then assessed in terms of (i)  $R_b$  as a function of  $m$ ; and (ii) the assigned  $b$  versus the order of  $m$ . Here, we have adopted the target BER of  $10^{-3}$  allowing a margin for the 7% forward error correction limit (FEC), which has a BER limit of  $3.8 \times 10^{-3}$  [39]. The  $\text{SNR}_{\text{threshold}}$  for the targeted BER can be found as the literature [40]. Therefore, at the target BER we defined a set of values for  $\text{SNR}_{\text{threshold}}$  of {6.8, 9.8, 16.6, 22.6, 28.5} dB for  $b = \{1, 2, 4, 6, 8\}$ , respectively.

Note that, the reported net data rate  $R_{net} = \sum_i^N R_{b,i}$ , where  $N$  is the channels (i.e., 4 in this case) with no 7% FEC overhead. Through sequential isolation of the LEDs, we measured that the inter-channel crosstalk to be  $< 0.2$  dB,

therefore the individual channels can be considered as a single-input single-output (SISO) link.

Following the above procedure, the  $m$ -CAP signals are transmitted and the BER is determined by comparing  $d'_d(t)$  and  $d_d(t)$ .

### III. RESULTS AND DISCUSSIONS

In this section, we outline experimental evaluation of a  $4 \times 4$  optical imaging MIMO-VLC utilising the  $m$ -CAP scheme by investigating the impact of using (i) different  $B_{sig}$ , while maintaining a fixed  $L$  of  $\sim 1$  m; (ii) a range of subcarriers  $m$  up to 20 and  $B_{sig}$  of 5, 10, 15 and 20 MHz for  $L$  of  $\sim 1$  m at the adopted BER target of  $10^{-3}$ ; and (iii) a range of  $L = \sim 1, 1.8$  and 4.5 m and  $m = \{20, 15, 10, 5\}$  for  $B_{sig}$  of 10 MHz.

#### A. Signal bandwidth $B_{sig}$

Fig. 4(a) illustrates  $R_{net}$  as a function of  $m$  for a range of  $B_{sig}$ , for  $L$  of  $\sim 1$  m and a BER of  $10^{-3}$ . Note, 20-CAP displays the highest  $R_{net}$  of  $\sim 249$  Mb/s (the highest reported in this work) at a BER of  $3.2 \times 10^{-3}$  for  $B_{sig} = 20$  MHz, which reduces to  $\sim 121$  Mb/s for  $B_{sig} = 5$  MHz. At the  $B_{sig}$  of 5 MHz, the increase in  $R_{net}$  as a function of  $m$  is relatively small since all the subcarriers have a similar bandwidth per subcarrier  $B_{sc}$ . For the  $B_{sig}$  of 20 MHz, the drop in  $R_{net}$  is due to reduced  $B_{sc}$  for a given  $m$  and  $B_{sig}$ . For example, for  $m = 20$  and  $B_{sig} = 20$  MHz, the  $B_{sc}$  is 1 MHz, whereas, for  $m = 20$  and  $B_{sig} = 5$  MHz,  $B_{sc}$  reduces to 0.25 MHz. For  $B_{sig}$  of 15 and 10 MHz,  $R_{net}$  reaches 237.75 Mb/s and 213.49 Mb/s, respectively. Moreover, for higher values of  $B_{sig}$  (e.g., 20 MHz and  $m = 20$ ) the out of band subcarriers can still be loaded with  $b = 4$  starting from the 7<sup>th</sup> subcarrier as shown in Fig. 4(b), which depicts the assigned  $b$  values for 20-CAP and for a range of  $B_{sig}$  {20, 15, 10 and 5 MHz}.

Using a range of  $B_{sig}$  (i.e., 20, 15, 10 and 5 MHz) for  $m = 20$ , we observe  $\eta_{net}$  of 12.45, 15.85, 21.34, 24.26 b/s/Hz, respectively. This is interesting as it shows that using higher  $B_{sig}$  leads to less utilisation of the spectrum but higher  $R_{net}$ . Moreover, for  $m = 20$  and  $B_{sig}$  of 5, 10 and 15 MHz we observe an improvement in  $\eta_{net}$  of  $\sim 95\%$ ,  $\sim 72\%$  and  $\sim 27\%$  compared to  $m = 20$  and  $B_{sig}$  of 20 MHz. Hence, there is a trade-off between the achievable  $R_{net}$  and spectral utilisation when considering different values of  $B_{sig}$  for the same  $m$ -CAP system. This can be attributed to the fact  $B_{sc}$  increases with  $B_{sig}$  since the subcarriers are divided equally, which leads to reduced SNR of each individual subcarrier positioned outside the pass-band region (i.e., the roll-off region of the LPF response of the LED with 20 dB/decade). Therefore, they are assigned with a low  $b$  value (see Fig. 4(b)). However, due to the increase in  $B_{sig}$  the  $R_{net}$  is boosted as it increases proportionally with  $B_{sig}$  (i.e.,  $\frac{1}{T_s}(1 + \beta)m$ ). Moreover,  $R_{net} = \sum_{i=1}^m k_i \frac{1}{T_s}$  for all four channels in addition to removal of the 7% FEC overhead. In contrast, for a given  $m$  decreasing  $B_{sig}$  leads to a higher SNR per subcarrier, which is due to lower  $B_{sc}$  that ensures higher  $b$  values (Fig. 4(b)). Therefore, achieving higher spectral utilisation for a given  $B_{sig}$ .

In Table II we have summarised the results in a tabular form for simplicity.



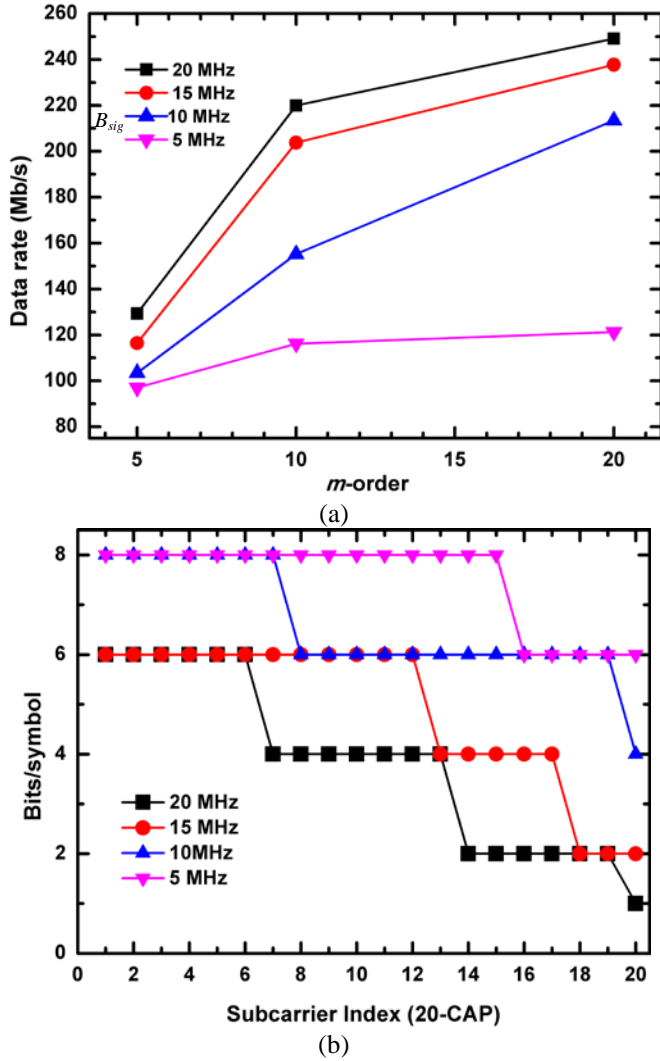


Fig. 4. (a) The net data rate  $R_{net}$  against  $m$  for a range of  $B_{sig}$ , and a BER of  $10^{-3}$ , and (b) assigned bits/symbol for 20-CAP for a range of  $B_{sig}$  (20, 15, 10 and 5 MHz). Note, in (b) the highest value of  $b = 8$  is assigned for the first 7<sup>th</sup> and 15<sup>th</sup> subcarriers with  $B_{sig}$  of 10 and 5 MHz, respectively, since they are within  $B_{LED}$

Table II: SUMMARY OF THE ACHIEVED  $R_{net}$  AND  $\eta_{net}$  FOR A RANGE OF  $B_{sig}$  AND  $m$

$m$	$B_{sig}$	5 MHz	10 MHz	15 MHz	20 MHz
5	$R_{net}$	97.03 Mb/s	103.5 Mb/s	116.44 Mb/s	129.39 Mb/s
	$\eta_{net}$	19.4 b/s/Hz	10.35 b/s/Hz	7.76 b/s/Hz	6.46 b/s/Hz
10	$R_{net}$	116.25 Mb/s	155.26 Mb/s	203.79 Mb/s	219.96 Mb/s
	$\eta_{net}$	23.25 b/s/Hz	15.52 b/s/Hz	13.58 b/s/Hz	11 b/s/Hz
20	$R_{net}$	121.31 Mb/s	213.49 Mb/s	237.75 Mb/s	249.07 Mb/s
	$\eta_{net}$	24.26 b/s/Hz	21.34 b/s/Hz	15.85 b/s/Hz	12.45 b/s/Hz

In order to demonstrate the performance of SISO under the same conditions as the imaging MIMO,  $R_{net}$  for a range of  $m = \{20, 15, 10, 5\}$ ,  $L$  of  $\sim 1$  m and a target BER of  $10^{-3}$  for one of the channels (i.e., Ch1) is shown in Fig. 5. Note that, as stated earlier all four channels in MIMO have the same data rate therefore, each channel can be considered as a SISO link. As

illustrated in Fig. 5, the highest  $R_{net}$  that can be supported by a SISO link is 62.26 Mb/s for  $m = 20$  and  $B_{sig} = 20$  MHz. For  $B_{sig} = 5$  MHz the  $R_{net}$  drops to 24.25 Mb/s, which is the lowest value reported for a SISO link. A summary of the achieved results for the SISO link for a range of  $m$  and  $B_{sig}$  is given in the Table III.

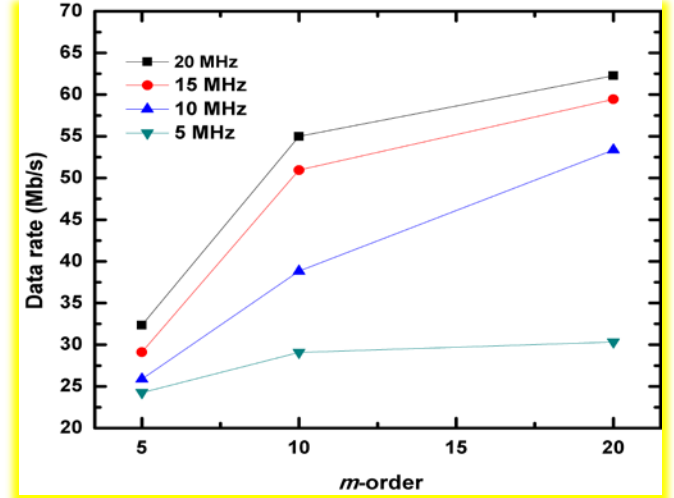


Fig. 5. The net data rate  $R_{net}$  against  $m$  for a range of  $B_{sig}$  for SISO (Ch1)

Figs. 6(a) and (b) depict the measured frequency spectra of the 20-CAP system for the  $B_{sig}$  of 20 MHz and the corresponding constellation diagrams of the 1<sup>st</sup> (black), 7<sup>th</sup> (red), and 14<sup>th</sup> (green) subcarriers, respectively. From Fig. 5(a) the 1<sup>st</sup> six subcarriers occupy a bandwidth of 6 MHz. Note,  $EVM_{RMS}$  values for the three constellations shown are 5.11%, 7.31% and 15.73%, respectively. Fig. 7 then illustrates the spectral efficiency as a function of  $m$  for the range of  $B_{sig}$ . Note, from Fig. 4(a) for  $m = 10$  and  $B_{sig}$  of 20, 15, 10 and 5 MHz, the  $R_{net}$  that can be supported are 219.96, 203.79, 155.26 and 116.25 Mb/s, respectively. This corresponds to  $\eta_{net}$  of 11, 13.58, 15.52 and 23.25 b/s/Hz for the listed  $B_{sig}$ . Moreover, improved spectral utilisation of  $\sim 130\%$ ,  $\sim 54\%$  and  $34.45\%$  for  $B_{sig}$  of 5, 10 and 15 MHz, respectively, is obtained in contrast to the  $B_{sig}$  of 20 MHz. For  $m = 5$  and  $B_{sig}$  of 20, 15, 10 and 5 MHz,  $\eta_{net}$  values are reduced to 6.46, 7.76, 10.35 and 19.4 b/s/Hz, respectively. Alternatively, for  $B_{sig}$  of 5, 10, and 15 MHz and  $m$  of 5 we observe corresponding improvement in the spectrum utilisation of 203%  $\sim 60\%$  and  $\sim 74\%$  compared to the  $B_{sig}$  of 20 MHz.

At this stage, it is worth mentioning that by combining both space multiplexing (MIMO) and frequency multiplexing ( $m$ -CAP) schemes, the overall system transmission speed is improved by  $\sim 8$  times from 31.53 Mb/s to  $\sim 249$  Mb/s in contrast to [26]. To the best of authors' knowledge this is the only experimental work on implementation of  $m$ -CAP (up to 10) in the VLC domain reported in the literature. We have kept  $L$  to be  $\sim 1$  m. However, in this work  $B_{sig}$  is increased by  $\sim 3$  times, which is higher than the 6.5 MHz adopted in [26]. It should be noted that, the aim of this paper is not to achieve the highest value in  $R_{nets}$ , but to demonstrate the possible gain that

can be achieved by combining space and frequency

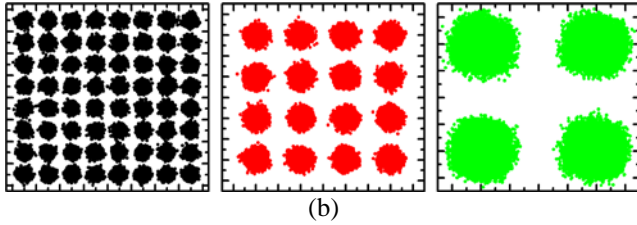
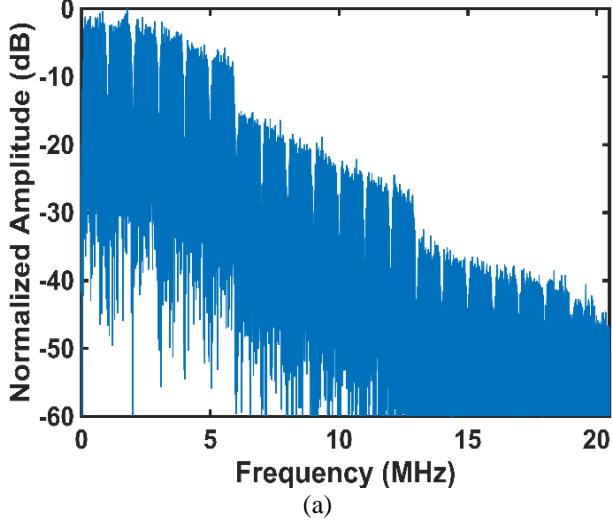


Fig. 6. 20-CAP with  $B_{sig}$  of 20 MHz; (a) the measured frequency spectrum, and (b) constellation diagrams for the 1<sup>st</sup>, 7<sup>th</sup> and 14<sup>th</sup> subcarriers

multiplexing schemes.

Table III: SUMMARY OF SISO'S ACHIEVED  $R_{net}$  AND  $\eta_{net}$  FOR DIFFERENT  $B_{sig}$  AND A RANGE OF  $m$

$m$	$B_{sig}$	5 MHz	10 MHz	15 MHz	20 MHz
5		24.25 Mb/s	25.87 Mb/s	29.11 Mb/s	32.34 Mb/s
		4.85 b/s/Hz	2.58 b/s/Hz	1.94 b/s/Hz	1.61 b/s/Hz
10		29.06 Mb/s	38.81 Mb/s	50.94 Mb/s	55 Mb/s
		5.81 b/s/Hz	3.88 b/s/Hz	3.39 b/s/Hz	2.75 b/s/Hz
20		30.32 Mb/s	53.37 Mb/s	59.43 Mb/s	62.26 Mb/s
		6.07 b/s/Hz	5.33 b/s/Hz	3.96 b/s/Hz	3.11 b/s/Hz

Moreover, in order to increase  $R_{net}$  we have doubled the  $m$ -order to 20, but at the cost of increased computational complexity of the overall system, since for every increment in  $m$ , 2 more pulse shaping FIR filters (i.e., one each for  $I$  and  $Q$ ) are required at both the Tx and the Rx. Note, increasing  $m$  from 10 to 20 will lead to the increase of the number of convolution operations from 460 to 1840 at the Tx. For MIMO-VLC  $m$ -CAP with  $m = 10$ ,  $R_{net}$  is increased to 213.49 Mb/s compared to 31.53 Mb/s [26] (i.e., a factor of 6.77) over the same  $L$  of 1 m. Increasing  $B_{sig}$  to 10 MHz results in  $\eta_{net}$  being increased by a factor of 4.4 as the obtained  $\eta_{net}$  is 21.34 b/s/Hz compared to 4.85 b/s/Hz in [26], which is considerable in VLC.

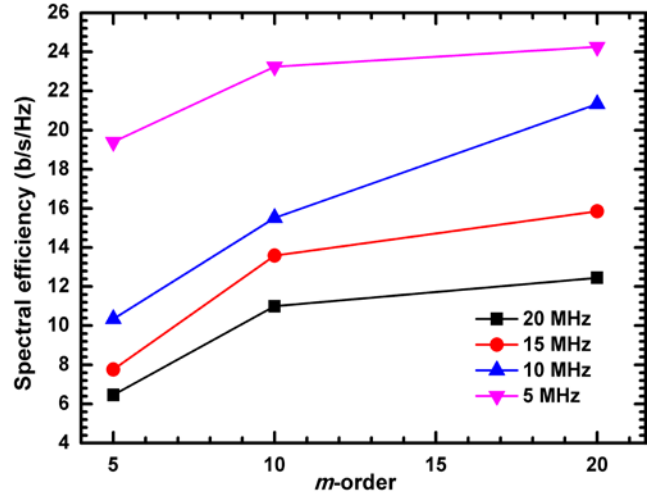


Fig. 7. The spectral efficiency against  $m$  for a range of  $B_{sig}$  {20, 15, 10 and 5 MHz}

### B. Transmission span

Fig. 8 illustrates  $R_{net}$  as a function of  $L$  for a range of  $m = \{20, 15, 10, 5\}$  and the  $B_{sig}$  of 10 MHz. In addition, the illuminance values at the Rx for the targeted  $L$  are also depicted in the figure. As expected, the illuminance value drops as  $L$  increases. The measured recorded illuminance values of 545, 190 and 82 lx are for  $L = \sim 1, 1.8$  and 4.5 m. As expected, with the increasing  $L$  from 1 to 4.5 m has reduced  $R_{net}$  from 213 Mb/s to approximately 50 Mb/s for 20-CAP. Therefore for 20-CAP this results in  $\eta_{net}$  of 21.35 b/s/Hz and 5 b/s/Hz for the BER values of  $1.2 \times 10^{-3}$  and  $3.7 \times 10^{-3}$ , respectively. For a range of  $m = \{20, 15, 10, 5\}$  and  $L$  of  $\sim 1$  m  $R_{net}$  values are 213.49, 181.14, 155.26 and 116.44 Mb/s, respectively; where the corresponding values of  $\eta_{net}$  are 21.35, 18.11, 15.52 and 11.64 b/s/Hz. Finally, Fig. 9 outlines the achievable BER performance as a function of  $L$  for a range of  $m$ . As expected, the BER increases with  $L$  and  $m$ , reaching  $3.7 \times 10^{-3}$ , which is still below the 7% FEC limit of  $3.8 \times 10^{-3}$  for  $m = 20$  and  $L$  of 4.5 m.

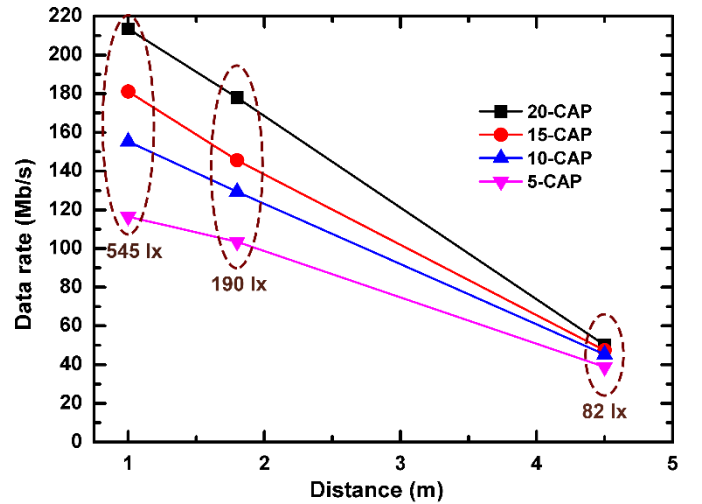


Fig. 8. The measured net data rate  $R_{net}$  as a function of the transmission distance for  $B_{sig}$  of 10 MHz and a range of  $m$ -CAPs. Illuminance values at the Rx for the tested transmission distances are also labelled in the figure

By extending  $L$  to 1.8 m,  $R_{net}$  is dropped to 177.9, 145.56, 129.39 and 103.5 Mb/s (see Fig. 8), which corresponds to a reduction in  $\eta_{net}$  of 17.79, 14.55, 12.94 and 10.35 b/s/Hz. The highest BER achieved for the  $L$  of 1.8 m is  $2.6 \times 10^{-3}$  at  $m = 20$  (see Fig. 9); following the same upward trend as in  $m$  and  $L$ .

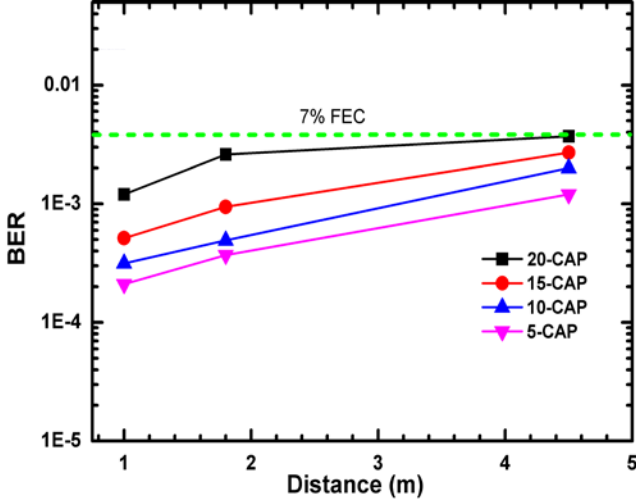


Fig. 9. The measured BER as a function of the distances for different values of  $m$ ; also included is the 7% FEC limit (dashed green)

For the highest  $L$  of 4.5 m,  $R_{net}$  is reduced (refer to Fig. 8) compared to the shorter distances, with  $R_{net}$  of 50.13, 47.43, 45.28 and 38.81 Mb/s at  $m = \{20, 15, 10, 5\}$ , respectively. Similar values of  $R_{net}$  are observed for lower values of  $b$  for each subcarrier. In other words, the bit loading algorithm fails to introduce any improvement in the overall  $R_{net}$  as a result of all subcarriers having low SNR values (i.e.,  $\ll 16.6$  dB; which is the  $SNR_{threshold}$  at  $b = 4$ ). Also, a reduction in the spectral efficiency was observed and for the first time in this work, it fell below 5 b/s/Hz. A summary of the achieved results for a set of  $L$  and  $m$  is provided in a tabular form for simplicity (see Table IV)

Table IV: SUMMARY OF THE ACHIEVED  $R_{net}$  AND  $\eta_{net}$  FOR A RANGE OF  $L$  AND  $m$

$L \backslash m$	$\sim 1$ m	1.8 m	4.5 m
5	116.44 Mb/s 11.64 b/s/Hz	103.5 Mb/s 10.35 b/s/Hz	38.81 Mb/s 3.88 b/s/Hz
10	155.26 Mb/s 15.52 b/s/Hz	129.39 Mb/s 12.94 b/s/Hz	45.28 Mb/s 4.52 b/s/Hz
15	181.14 Mb/s 18.11 b/s/Hz	145.56 Mb/s 14.55 b/s/Hz	47.43 Mb/s 4.74 b/s/Hz
20	213.49 Mb/s 21.35 b/s/Hz	177.9 Mb/s 17.79 b/s/Hz	50.13 Mb/s 5 b/s/Hz

#### IV. CONCLUSION

In this paper, we have reported for the first time, an investigation of the performance of a  $4 \times 4$   $m$ -CAP imaging MIMO (i.e., frequency and space multiplexing) VLC link considering a range of system parameters. By combining the

two schemes, we experimentally demonstrated an improvement in the transmission speed reaching a maximum value of  $\sim 249$  Mb/s. We showed that there is a trade-off between  $R_{net}$  and  $\eta_{net}$ , since for a given values of  $m$  and  $L$  increasing  $B_{sig}$  substantially improved  $R_{net}$ ; however, interestingly  $\eta_{net}$  was reduced. Moreover, the highest  $R_{net}$  of 249.07 Mb/s was achieved at a BER of  $3.2 \times 10^{-3}$  for  $B_{sig}$  of 20 MHz and for  $m = 20$  over a transmission span of  $\sim 1$  m. On the other hand, for lower  $B_{sig}$  of 5 MHz and for  $m = 20$  the achieved  $R_{net}$  was reduced to 121.21 Mb/s, but spectrum utilisation was almost 95% better in contrast to  $B_{sig}$  of 20 MHz. We also observed that for a given value of  $m$  and  $B_{sig}$ , increasing the distance resulted in reduced  $R_{net}$ . The overall  $R_{net}$  ( $\eta_{net}$ ) for all proposed system (i.e., four channels) were 213.49 Mb/s (21.35 b/s/Hz), 177.9 Mb/s (17.79 b/s/Hz), and 50.13 Mb/s (5.01 b/s/Hz) for  $m = 20$  and the  $B_{sig}$  of 10 MHz over a range of  $L$  (i.e.,  $\sim 1$  m, 1.8 m and 4.5 m), respectively, at BER values of  $1.2 \times 10^{-3}$ ,  $2.6 \times 10^{-3}$ , and  $3.7 \times 10^{-3}$ .

Moreover, we showed that for the highest  $L$  of 4.5 m increasing  $m$  did not introduce any significant improvement in the system performance, but increased the computational complexity by the way of increased number of the pulse shaping FIR filters. In our future work, we will experimentally compare the  $m$ -CAP and OFDM schemes performance.

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